Circuit breaker provides overcurrent and precise overvoltage protection

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Requiring only a handful of inexpensive components, the circuit breaker in Figure 1 responds to both overcurrent- and overvoltage-fault conditions. At the heart of the circuit, $D_2$, an adjustable, precision, shunt-voltage regulator, provides a voltage reference, comparator, and open-collector output, all integrated into a three-pin package.

Figure 1 This circuit breaker provides both overvoltage and overcurrent protection. Other than the current flowing in $R_3$, $R_4$, and $D_2$'s cathode, the circuit draws no current from the supply in its normal untripped state.

Figure 2 shows a simplified view of the ZR431, $D_1$. The voltage appearing at the reference input is compared with the internal voltage reference, $V_{REF}$, nominally 2.5V. In the off state, when the reference voltage is 0V, the output transistor is off, and the cathode current is less than 0.1 µA. As the reference voltage approaches $V_{REF}$, the cathode current increases slightly; when the reference voltage exceeds the 2.5V threshold, the device fully switches on, and the cathode voltage falls to approximately 2V. In this condition, the impedance between the cathode and the supply voltage
determines the cathode current; the cathode current can range from 50 µA to 100 mA.

**Figure 2** In this simplified view of the ZR431, the voltage at its reference input is compared with the internal voltage reference, which is nominally 2.5V.

Under normal operating conditions, $D_2$’s output transistor is off, and the gate of P-channel MOSFET $Q_4$ goes through $R_9$, such that the MOSFET is fully enhanced, allowing the load current, $I_{LOAD}$, to flow from the supply voltage, $-V_S$, through $R_6$ into the load. $Q_2$ and current-sense resistor $R_6$ monitor the magnitude of $I_{LOAD}$, where $Q_2$’s base-emitter voltage, $V_{BE}$, is $I_{LOAD} \times R_6$. For normal values of $I_{LOAD}$, $V_{BE}$ is less than the 0.6V necessary to bias $Q_2$ on, such that the transistor has no effect on the voltage at the junction of $R_3$ and $R_4$. Because the input current at $D_2$’s reference input is less than 1 µA, negligible voltage drops across $R_5$, and the reference voltage is effectively equal to the voltage on $R_4$.

In the event of an overload when $I_{LOAD}$ exceeds its maximum permissible value, the increase in voltage across $R_6$ results in sufficient base-emitter voltage to turn on $Q_2$. The voltage on $R_4$ and, hence, the reference voltage now pull up toward $V_S$, causing $D_2$’s cathode voltage to fall to approximately 2V. $D_2$’s output transistor now sinks current through $R_7$ and $R_8$, thus biasing $Q_3$ on. $Q_3$’s gate voltage now effectively clamps to the supply voltage through $Q_3$, and the MOSFET turns off. At the same instant, $Q_3$ sources current into $R_4$ through $D_1$, thereby pulling the voltage on $R_4$ to a diode drop below the supply voltage. Consequently, no load current flows through $R_6$, because $Q_2$’s base-emitter voltage is now 0V, has turned off. As a result, no load current flows through $R_6$. $D_2$’s output transistor latches on, and the circuit remains in its tripped state in which the load current is 0A. When choosing a value for $R_6$, ensure that $Q_2$’s base-emitter voltage is less than approximately 0.5V at the maximum permissible value of the load current.

As well as responding to overcurrent conditions, the circuit breaker also reacts to an abnormally large value of the supply voltage. When the load current lies within its normal range and $Q_2$ is off, the magnitude of the supply voltage and the values of $R_3$ and $R_4$, which form a potential divider across the supply rails, determine the voltage at the reference input. In the event of an overvoltage at the supply voltage, the voltage on $R_4$ exceeds the 2.5V reference level, and $D_2$’s output transistor turns on. Once again, $Q_3$ turns on, MOSFET $Q_4$ switches off, and the load becomes effectively isolated from the dangerous transient.

The circuit now remains in its tripped state until reset. Under these conditions, $Q_3$ clamps $Q_4$’s gate-source voltage to roughly 0V, thereby protecting the MOSFET itself from excessive gate-source voltages. Ignoring the negligibly small voltage across $R_5$, you can see that the reference voltage is $V_S \times R_4/(R_3+R_4)$ in volts. Because $D_2$’s output turns on when the reference voltage exceeds 2.5V, you can rearrange the equation as $R_4 = (V_S/2.5-1) \times R_4$ in ohms, where $V_S$ is the required supply-voltage trip level. For example, if $R_4$ has a value of 10 kΩ, a trip voltage of 18V would require $R_4$ to have a
value of 62 kΩ. When choosing values for R₃ and R₄ to set the desired trip voltage, ensure that they are large enough that the potential divider will not excessively load the supply. Similarly, avoid values that could result in errors due to the reference-input current.

When you first apply power to the circuit, you’ll find that capacitive, bulb-filament, motor, and similar loads having large inrush current can trip the circuit breaker, even though their normal, steady-state operating current is below the trip level that R₆ sets. One way to eliminate this problem is to add capacitor C₂, which slows the rate of change of the voltage at the reference input. However, although simple, this approach has a serious disadvantage in that it slows the circuit’s response time to a genuine overcurrent-fault condition.

Components C₁, R₁, R₂, and Q₁ provide an alternative solution. On power-up, C₁ initially discharges, causing Q₁ to turn on, thereby clamping the reference input to 0V and preventing the inrush current from tripping the circuit. C₁ then charges through R₁ and R₂ until Q₁ eventually turns off, releasing the clamp at the reference input and allowing the circuit to respond rapidly to overcurrent transients. With the values of C₁, R₁, and R₂, the circuit allows approximately 400 msec for the inrush current to subside. Selecting other values allows the circuit to accommodate any duration of inrush current you apply to a load. Once you trip the circuit breaker, you can reset it either by cycling the power or by pressing S₁, the reset switch, which connects across C₁. If your application requires no inrush protection, simply omit C₁, R₁, R₂, and Q₁ and connect S₁ between the reference input and 0V.

When choosing components, make sure that all parts are properly rated for the voltage and current levels they will encounter. The bipolar transistors have no special requirements, although these transistors, especially Q₂ and Q₃, should have high current gain, Q₄ should have low on-resistance, and Q₄’s maximum drain-to-source and gate-to-source voltages must be commensurate with the maximum value of supply voltage. You can use almost any small-signal diode for D₁. As a precaution, it may be necessary to fit zener diodes D₃ and D₄ to protect D₂ if extremely large transient voltages are likely.

Although this circuit uses the 431 device, which is widely available from different manufacturers, for D₂, not all of these parts behave in exactly the same way. For example, tests on a Texas Instruments TL431CLP and a Zetex ZR431CL reveal that the cathode current is 0A for both devices when the reference voltage is 0V. However, gradually increasing the reference voltage from 2.2 to 2.45V produces a change in cathode current ranging from 220 to 380 µA for the TL431CLP and 23 to 28 µA for the ZR431CL—roughly a factor of 10 difference between the two devices. You must take this difference in the magnitude of the cathode current into account when selecting values for R₇ and R₈.

The type of device you use for D₂ and the values you select for R₇ and R₈ can also have an effect on response time. A test circuit with a TL431CLP, in which R₇ is 1 kΩ and R₈ is 4.7 kΩ, responds within 550 nsec to an overcurrent transient. Replacing the TL431CLP with a ZR431CL results in a response time of approximately 1 µsec. Increasing R₇ and R₈ by an order of magnitude to 10 and 47 kΩ, respectively, produces a response time of 2.8 µsec. Note that the relatively large cathode current of the TL431CLP requires correspondingly small values of R₇ and R₈.

To set the overvoltage-trip level at 18V, R₃ and R₄ must have values of 62 and 10 kΩ, respectively. The test circuit then produces the following results: Using a TL431CLP for D₂, the circuit trips at 17.94V, and, using a ZR431CL for D₂, the trip level is 18.01V. Depending on Q₂’s base-emitter voltage, the overcurrent-detection mechanism is less precise than the overvoltage function. However, the overcurrent-detection accuracy greatly improves by replacing R₈ and Q₂ with a high-side current-sense amplifier that generates a ground-referred current proportional to load current. These devices are available from Linear Technology, Maxim, Texas Instruments, Zetex, and others.
The circuit breaker should prove useful in applications such as automotive systems that require overcurrent detection to protect against faulty loads and that also need overvoltage protection to shield sensitive circuitry from high-energy-load-dump transients. Other than the small current flowing in R₃ and R₄ and the current in D₂’s cathode, the circuit draws no current from the supply in its normal, untripped state.

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